

VOLTAGE SUPPLYING DEVICE, AND SEMICONDUCTOR DEVICE,
ELECTRO-OPTICAL DEVICE AND ELECTRONIC INSTRUMENT USING THE SAME

BACKGROUND OF THE INVENTION

5 Field of the Invention

The present invention relates to a voltage supplying device, and a semiconductor device, an electro-optical device and an electronic instrument using the voltage supplying device.

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Description of Related Art

In recent years, there are devices requiring a highly accurate voltage supply, for example, a liquid crystal display.

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In an active matrix type of liquid crystal display or a simple matrix type of liquid crystal display, the number of grayscales (or colors) of a liquid crystal panel is highly improved, and a voltage to be applied is developed to be more precise.

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In order to increase the number of grayscales of a liquid crystal panel, a thin film transistor (TFT) liquid crystal device which is an active matrix type of liquid crystal display uses three colors of RGB (red, green and blue) which includes data signals constituted of 6-bit data (64 grayscales, ca. 260,000 colors) or 8-bit data (256 grayscales, ca. 16,770,000 colors), for example.

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With the increase in the number of grayscales, a technique of setting a voltage level more precisely is required.

According to the characteristics in relationship between the applied voltage and the panel transmittance of a liquid crystal panel, the rate of change in panel transmittance with respect to the applied voltage is large where the transmittance is in the middle level around 50%, and is decreased when the panel transmittance approaches 100% or 0%. Therefore, in the region where the panel transmittance is in the middle level, a slight deviation in the applied voltage has a great influence on a gray level. In order to suppress the change in panel transmittance, a voltage to be applied to liquid crystal is required to be supplied more precisely.

The maximum permissible level in dispersion of a voltage to be applied to liquid crystal is ± 5 mV for 64 grayscales and ± 1 to ± 2 mV for 256 grayscales, for example, and more precise voltage is required to be applied to liquid crystal when the number of grayscales is increased. Although the dispersion in the threshold voltage V_{TH} of an ordinary IC chip is allowed to range from several tens mV to several hundreds mV, a liquid crystal display with the increased number of grayscales has a severer maximum permissible level. It can be predicted that further increase in the number of grayscales in future requires more precise setting method for a voltage to be applied to liquid crystal.

Consequently, there are conventionally various method of generating grayscale voltages in a driving circuit of a liquid crystal panel, such as a voltage selecting method, a time sharing method, or a digital-analog conversion method.

Fig. 4 shows a conventional voltage supplying device of the method using a digital-analogue conversion device (hereinafter referred to as a DAC method).

A voltage follower circuit 72, into which an output from a DAC 70 is entered, functions as an impedance converter, and in the case of a voltage follower circuit 72 in an ideal state, a voltage of a node 201 entered into a non-inverse input terminal becomes equal to a voltage of a node 202 entered into an inverse input terminal. However, conventionally in the voltage follower circuit 72 not compensated by an offset canceling circuit, an offset is formed between the input and the output due to dispersion in performance of respective transistors, so as to form a difference in voltage between the node 201 and the node 202.

Fig. 4 shows a voltage supplying device for solving the problem. The output from the DAC 70 is supplied to the non-inverse input terminal 201 of the voltage follower circuit 72, and the output of the voltage follower circuit 72 is returned to the inverse input terminal 202. In the course of the circuit connecting the output line and the non-inverse input terminal 201, a switching element Q10, a capacitance C10 and a switching element Q12 are connected in series. On the negative feedback line connected to the inverse input terminal 202, only a switching element Q1 is present. The switching element Q10 is connected in parallel to the capacitance C10 and the switching element Q11.

In a first period, the switching element Q11 is off, and

the switching element Q10 and the switching element Q12 are on, whereby an offset voltage between the input and the output of the voltage follower circuit 72 is charged in the capacitance C10. In a second period, the switching element Q11 is on, and
5 the switching element Q10 and the switching element Q12 are off, whereby a charge of offset canceling charged in the capacitance C10 is superposed and returned to the inverse input terminal 202 of the voltage follower circuit 72.

According to the foregoing manner, the offset is
10 cancelled out by applying a reverse voltage corresponding to the offset in such a manner that the capacitance C10 for offset canceling is provided on the circuit connecting the output line and the non-inverse input terminal 201 of the voltage follower circuit 72.

15 In the data driver of the conventional DAC method shown in Fig. 4, the capacitance C10 as the offset canceling circuit is necessarily housed in the chip. However, it requires a large area since the capacitance C10 having a sufficiently larger capacity than the input capacity of the voltage follower circuit
20 72. When the offset canceling capacity is too small, it is regarded as a noise in the input capacity of the voltage follower circuit 72, and thus the noise is superposed on the output voltage.

Furthermore, in order to charge the offset voltage in the
25 offset canceling capacitance C10, a period of time of from 3 to 5 μ s is generally required.

In the active matrix type of liquid crystal display of

these kinds, the horizontal scanning period (select period) is necessarily set at a short period when high definition display is conducted by increasing the number of pixels in one line. For example, the select period becomes as short as from 8 to 12 μ m in high definition display of SXGA.

In this case, it becomes difficult to assure a period of time for offset canceling when the period for charging the capacitance C10 for offset canceling occupies the select period.

BRIEF SUMMARY OF THE INVENTION

The invention has been developed taking the problems into consideration, and an objective thereof is to provide a voltage supplying device that can promptly and precisely provide a required charging voltage without an offset canceling circuit, and a semiconductor device, an electro-optical device and an electronic instrument using the same.

According to one aspect of the present invention, there is provided a voltage supplying device which supplies a voltage to a load capacitance to finish charging the load capacitance with a predetermined voltage within a predetermined charging period. The voltage supplying device may include: a reference voltage generating circuit having a ladder resistance circuit to which a plurality of resistors are connected in series, which outputs a plurality of voltages divided in the ladder resistance circuit as a plurality of gamma-corrected reference voltages; a plurality of first impedance conversion circuits which

perform impedance conversion on the plurality of reference voltages from the reference voltage generating circuit and output the converted voltages; a voltage selection circuit having a plurality of analogue switches one of which is turned
5 on based on grayscale data, which selects one of the plurality of reference voltages from the plurality of first impedance conversion circuits; a second impedance conversion circuit which performs impedance conversion on a voltage from the voltage selection circuit and outputs the converted voltage;
10 a first switching element for blocking an output of the second impedance conversion circuit; a first bypass line for shorting input and output lines of the second impedance conversion circuit; a second switching element provided on the first bypass line; a plurality of third switching elements for blocking an
15 output of the plurality of first impedance conversion circuits; a plurality of second bypass lines for shorting input and output lines of the respective plurality of first impedance conversion circuits; and a plurality of fourth switching elements provided on the respective plurality of second bypass lines.

20 Furthermore, the first switching element is turned on and the second switching element is turned off in the first period of the charging period, and the first switching element is turned off and the second switching element is turned on in the second period of the charging period which follows after the
25 ~~first period.~~

According to one aspect of the present invention, the output voltage from the second impedance conversion circuit is

supplied to the load capacitance through the first switching
element in the first period of the charging period. If an offset
is present between the input and output voltages of the second
impedance conversion circuit, the load capacitance will not be
5 charged with the predetermined voltage even when the output
voltage from the second impedance conversion circuit is
continuously supplied to the load capacitance.

Thus, the route for voltage supplying is switched to the
first bypass route in the second period of the charging time,
10 whereby the voltage from the voltage selection circuit is
directly supplied to the load capacitance without using the
second impedance conversion circuit. Accordingly, the load
capacitance is supplied with a voltage compensating the
shortage caused by the offset and can be charged with the
15 predetermined voltage. The charge amount per unit period of
time supplied from the voltage selection circuit to the load
capacitance is decreased since the impedance conversion is not
performed. However, if the load capacitance has been charged
with a sufficient voltage by the output voltage from the second
20 impedance conversion circuit, the load capacitance can be
charged to the predetermined voltage within the charging
period.

According one aspect of the present invention, the
plurality of third switching elements are turned on and the
25 plurality of fourth switching elements are turned off in the
first period of the charging period. As a result, a plurality
of reference voltages from the reference voltage generating

circuit are current-amplified in the plurality of first impedance conversion circuits. Accordingly, the total resistant value of the ladder resistance circuit of the reference voltage generating circuit is increased and current
5 flowing therethrough is reduced so as to reduce power consumption. At the same time, sufficient current can be supplied to analogue switches having load capacitance.

According to one aspect of the present invention, the plurality of third switching elements are turned off and the
10 plurality of fourth switching elements are turned off at least in a final stage of the second period in order to form a second bypass route. Further, the plurality of third switching elements are turned on and the plurality of fourth switching elements are turned off in the other periods of the charging
15 period. Since input/output offset is caused also in the plurality of first impedance conversion circuits, the offset can be cancelled at least in the last stage of the second period. Here, a node connected to ladder resistors and a node of output voltages are shorted. Therefore, even when the output voltages
20 are set into non-reference voltages, the output voltages are charged/discharged in the ladder resistors and can be reset into proper reference voltages.

According to one aspect of the present invention, because a capacitance for offset canceling used in the conventional
25 technique is not necessary, a period of time for charging the capacitance for offset canceling with an offset voltage is not necessary.

According to one aspect of the present invention, there may be a period in which both the first and second switching elements are turned off. This makes it possible to prevent positive feed back of the voltage from the voltage supplying source through the first bypass line to the impedance conversion circuit.

According to one aspect of the present invention, the voltage supplying device may further comprise a fifth switching element connected to a power supply line which supplies a power source voltage to the plurality of first impedance conversion circuit. The fifth switching circuit is turned off in synchronization with the off operation of the third switching element.

The voltage supplying device may further comprise a sixth switching element connected on a power source line which supplies a power source voltage to the second impedance conversion circuit. The sixth switching element is turned off, synchronized with an off operation of the first switching element. This makes it possible to stop the power supply when the output from the first and second impedance conversion circuits is unnecessary, so as to reduce power consumption.

The second conversion circuit used in one aspect of the present invention may be formed of a voltage follower circuit. When an input voltage having a magnitude near a power source potential VDD or a ground potential VEE is input to the voltage follower circuit, such voltage follower circuit has a property in which an output voltage is saturated and shows no linear

characteristics in response to an input voltage. In this case,
a voltage from the voltage supplying source is supplied to the
load capacitance through the bypass line by turning off the
first switching element and turning on the second switching
5 element in a saturated region of an output voltage of the voltage
follower circuit. This makes it possible to supply a linear
output voltage by directly outputting a voltage from the voltage
supplying source in the saturated region in which an output
voltage is saturated with respect to a lower or higher input
10 voltage in the voltage follower circuit.

According to one aspect of the present invention, there
is provided a semiconductor device comprising the above-
described voltage supplying device. In the semiconductor
device, a capacitance for offset canceling is unnecessary, so
15 that the chip size can be reduced by the area of the capacitance
or other element can be integrated on the area of the capacitance
to increase the degree of integration.

According to one aspect of the present invention, there
is provided an electro-optical device comprising a display
20 section using an electro-optical element and a semiconductor
device which is provided with the above- described voltage
supplying device, wherein the semiconductor device is used as
a driver IC for driving a signal line of the display section.
A precise driving voltage can be supplied to the electro-optical
25 element by supplying a voltage from the voltage supplying source
through a signal line of the display section to the
electro-optical element.

In this case, the electro-optical element may be driven based on grayscale voltages from the voltage supplying device. The voltage selection circuit can be formed of a digital-analogue converter which converts a digital grayscale signal to an analogue voltage. The first period of the charging period may be finished after the load capacitance is charged with a voltage which has a magnitude within a range corresponding to half of the least signification bit with respect to a desired grayscale voltage value to be supplied to the electro-optical element and which has a magnitude of 90% or more of the desired grayscale voltage value. When a sufficient voltage is supplied to the electro-optical element in the first period of the charging period, the applied voltage to the electro-optical element can reach the desired grayscale voltage even when the voltage from the DA converter is directly supplied to the load capacitance in the second period of the charging period, and furthermore, the gray level in the electro-optical element can be prevented from being differentiated.

According to one aspect of the present invention, there is provided an electronic instrument comprising the above-described electro-optical device. Image quality can be improved by using the electro-optical device as a display of the electronic instrument.

According to one aspect of the present invention, there are provided a plurality of impedance conversion circuits between a reference voltage supplying circuit and a reference voltage generating circuit. The above-described two switching

elements and bypass line are connected to the plurality of impedance conversion circuits.

BRIEF DESCRIPTION OF THE DRAWINGS

5 Fig. 1 is a schematic diagram showing a liquid crystal device to which the present invention is applied.

Fig. 2 is a block diagram showing a conventional data driver IC.

10 Fig. 3 is a graph showing the output characteristics of the conventional data driver IC shown in Fig. 2

Fig. 4 is a diagram showing an example of a voltage supplying device using a conventional voltage follower circuit shown in Fig. 2.

15 Fig. 5 is a diagram showing a voltage supplying device of the first embodiment of the invention.

Fig. 6A is a waveform chart showing operations of the voltage supplying device of Fig. 4, and Fig. 6B is a waveform chart showing operations of the voltage supplying device of Fig. 5.

20 Fig. 7 is a graph showing a relationship between the voltages charged in the liquid crystal capacitance in the first and second periods of the select period.

Fig. 8 is a diagram showing a voltage supplying device of the second embodiment of the invention.

25 Fig. 9 is a waveform chart showing operations of the voltage supplying device of Fig. 8.

Fig. 10 is a diagram showing a voltage supplying device

of the third embodiment of the invention.

Fig. 11 is a graph showing the input and output characteristics of the voltage follower circuit used in the fourth embodiment of the invention.

5 Fig. 12 is a circuit diagram of the voltage follower circuit having the characteristics shown in Fig. 11.

Fig. 13 is a diagram showing a voltage supplying device of the fourth embodiment of the invention containing the voltage follower circuit shown in Fig. 12.

10 Fig. 14 is a diagram showing a modified example of the voltage supplying device shown in Fig. 13.

Fig. 15 is a diagram showing a voltage supplying device of the fifth embodiment of the invention.

15 Fig. 16 is a diagram showing a voltage supplying device according to a sixth embodiment of the present invention.

Fig. 17 is a diagram showing a connecting state of the device shown in Fig. 16 in a first period.

Fig. 18 is a diagram showing a connecting state of the device shown in Fig. 16 in a second period.

20 Fig. 19 is a diagram showing a reference voltage supplying circuit that is an essential part of a voltage supplying device according to a seventh embodiment of the present invention.

DETAILED DESCRIPTION OF THE PREFERRED EMBODIMENTS

25 Preferred embodiments of the invention will be described below with reference to the drawings.

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First Embodiment

Liquid Crystal Device

Fig. 1 shows a construction diagram of the whole body of a liquid crystal device including a liquid crystal panel device
5 and peripheral circuits thereof.

In Fig. 1, a liquid crystal panel 20 is, for example, a TFT type of liquid crystal panel.

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A gate driver IC 40 (scanning line driver IC) connected to address lines (scanning lines) and a data driver IC 30 (signal line driver IC) connected to data lines (signal lines) are provided as a circuit driving the liquid crystal panel 20. The gate driver IC 40 and the data driver IC 30 are supplied with predetermined voltages from a power source circuit 46 and drive the data lines 21 and gate lines 22 based on the signals supplied from a signal control circuit 42. The data driver IC 30 and the gate driver IC 40 each is actually constituted by plural ICs. A grayscale voltage circuit 44 supplies a reference voltage necessary for driving based on grayscale voltages in the data driver IC 30. A liquid crystal capacitance 25 is formed
20 by sealing a liquid crystal between a pixel electrode 24 and a common electrode 23. A common electrode driving circuit 48 supplies a common voltage to the common electrode 23.

The invention is not limited to a TFT type of liquid crystal panel but can be applied to other display panels using
25 an electro-optical element including a liquid crystal.

Data Line Driving Circuit

Fig. 2 is a constitution diagram of the data driver IC 30 for driving the liquid crystal panel 20 shown in Fig. 1, and Fig. 3 is an example of a driving wave form driving the data line 21 in the liquid crystal panel 20 shown in Fig. 1.

5 Fig. 2 is a internal block diagram of the data driver IC 30 for displaying three colors and 64 grayscales, for example, having 300 output lines as the data line output 21.

In the data driver IC 30, display data composed of RGB signals each having 6 bits supplied from the signal control circuit 42 is latched by an input latch circuit 50 one by one based on the timing of a clock signal $\phi 1$ similarly supplied from the signal control circuit 42. The display data corresponding to 100 clocks of the clock signal $\phi 1$ (RGB x 6 bits x 100 clocks) is incorporated in a line latch circuit 52 through a 100-bit shift register 51. The display data is further incorporated in a latch circuit 53 at the timing of a latch pulse LP. The display data in the latch circuit 53 is converted to an analogue signal by a 6-bit DAC 54 and further subjected to impedance conversion by a voltage follower circuit 55, whereby it is supplied to the data lines 21 of the liquid crystal panel 20.

As shown in Fig. 3, the 6-bit DAC 54 generates 64 levels of grayscale voltage, and for example, 10 levels of voltages V1 to V10 are supplied from the outside. The reference voltages V1 to V10 are supplied from the grayscale voltage circuit 44. In the DAC 54, for example, one of the voltages in the voltage range divided into 10 levels of reference voltage V1 to V10 is

selected by the upper three bits of each 6 bits of RGB. For example, a reference voltage between V4 and V5 is selected. Then, V34 level, which is one of the eight voltage levels in the voltage range specified by the upper three bits, for example, the voltage range between V4 and V5, is selected by the lower three bits of the data.

Voltage Supplying Device

Fig. 5 shows a circuit diagram of a voltage supplying device 58 outputting an output of a DAC 70 to the data lines of the TFT type of liquid crystal panel through a voltage follower circuit 72.

The DAC 70 shown in Fig. 5 is connected to one data lines 21, and the DA converter 54 shown in Fig. 2 is constituted by plural DACs 70. The relationship between the voltage follower circuit 72 and the voltage follower circuit 55 is the same.

In the circuit shown in Fig. 5, the output from the DAC 70 is supplied to a non-inverse input terminal 201 of the voltage follower circuit 72, and the output of the voltage follower circuit 72 is returned and supplied to an inverse input terminal 202. A first switching element Q1 is provided on an output line between the voltage follower circuit 72 and a load capacitance (a wiring capacitance of the data lines 21 or the liquid crystal capacitance 25). A second switching element Q2 is provided on a bypass line 205 supplying the voltage from the DAC 70 to the load capacitance bypassing the voltage follower circuit 72 and the first switching element Q1.

A control signal from a first control signal generation circuit 74 is supplied to the second switching element Q2 for on-off control. An inverter INV1 is connected to the first switching element Q1 to supply an inverse signal of the output from the first control signal generation circuit 74, so as to subject the first switching element Q1 to on-off control. The control signal is, for example, a signal CNT1 output based on the timing synchronized with the latch pulse LP of the data shown in Fig. 6B described later.

Fig. 6A shows wave forms of the latch pulse LP, the supplied voltages VX1 and VX 2 to the gate lines, and an output voltage to the data lines. Within the period of one frame, the voltage wave form charged in the liquid crystal capacitance 25 through the data line 21 in the select period of the gate line 22 is shown by VY1.

A voltage applied to the data lines 21 is demanded to have high accuracy with the increase in the number of grayscales and colors of the current liquid crystal panels. But conventionally, a potential output through the voltage follower circuit does not reach the necessary grayscale potential due to dispersion of the input and output voltages caused by offset, so that it is often difficult to set the grayscale potential in a highly accurate manner.

That is, as shown in Fig. 6A, it does not reach the grayscale potential within the select period t , and the potential short by δ is charged in the liquid crystal capacitance 25. The variation of the input and the output caused by the

offset can be compensated by providing the offset canceling circuit as shown in Fig. 4, but it brings about such problems that the area of the capacitance C10 therefor is increased, and the speed of attaining the necessary grayscale potential is insufficient.

According to the embodiment, taking the limitation in output performance of the voltage follower circuit into consideration, switching is conducted, at a time when the grayscale potential output can be maintained to a certain extent, in such a manner that the output from the DAC 70 is supplied to the liquid crystal capacitance 25 instead of the output of the voltage follower circuit.

In Fig. 6B, operation of the data driver of the TFT type of liquid crystal panel device relating to the embodiment will be described below with reference to Fig. 5.

While varying depending on the specifications, it takes about a half of the select period to amplify the output of the voltage follower circuit 72 by the DAC method of the TFT type of liquid crystal device to 99% or more of the necessary voltage value. For example, in the case of the liquid crystal driver requiring 12 V, the charge amount $Q = 12 \times C$ (C represents a load capacitance) is necessarily charged by the output of the voltage follower circuit 72. When the difference between the input voltage and the output voltage at the end of the first period of the select period reaches 10 mV, the load capacitance (charge amount) that should be charged in the second period of the select period is $Q = 0.01 \times C$. As a result, in the case

of switching to the output of the DAC 70, the necessary grayscale voltage can be obtained by supplying a charge amount of $1/1,200$ (about 0.1%) of the necessary charge amount Q . While the select period t varies depending on the panels, it is generally about
5 from 8 to 12 μs for high definition display of SXGA.

A voltage $VX1$ is applied to one of the gate lines 21 by the gate driver IC40 over the select period t between the latch pulses LP, so as to turn the transistor on. According the procedure, the liquid crystal capacitance 25 in the liquid
10 crystal panel 20 falls in the chargeable state. In the data driver IC30, the first switching element Q1 is turned on, and the second switching element Q2 is turned off by the control signal CNT1 output in synchronized with the latch pulses LP. Thus, a voltage $VY2$ is output from the voltage follower circuit
15 72 to the data lines 21. The voltage $VY2$ is charged in the liquid crystal capacitance 25 through the data lines 21, and the charge in the liquid crystal capacitance 25 shows such change in lapse of time that it reaches, for example, the point A exceeding 99% of the necessary voltage within the first period $t1$.

20 In the second period $t2$, the first switching element Q1 is turned off, and the second switching element Q2 is turned on, whereby the output of the voltage follower circuit 72 is cut off, so as to directly charge the output of the DAC 70 in the liquid crystal capacitance 25 through the data lines 21.

25 In the DAC 70 at this time, while the charge amount that can be supplied per unit period of time is small, the active load influencing the output voltage is small, and the charge of the

liquid crystal capacitance 25 is substantially completed, whereby the sufficient voltage can be charged in the liquid crystal capacitance 25 within the select period t .

In the case where, for example 10 mV is generated as the offset between the input and the output of the voltage follower circuit 72, switching is necessarily conducted before the necessary grayscale voltage by 10 mV. While depending on the design of the proportion between the electric current driving performances of the voltage follower circuit 72 and the DAC 70, it is appropriate to set the switching time at the time when the point A in Fig. 6B reaches 99% of the necessary voltage when the proportion is 1/100.

As described in the foregoing, in the first period t_1 of the select period t , a larger charge amount per unit period of time is supplied by the output of the voltage follower circuit 72 to charge the liquid crystal capacitance 25 to a voltage of certain level. In the second period t_2 of the select period t , the output of the DAC 70 is directly supplied to the liquid crystal capacitance 25, whereby a highly accurate output voltage can be rapidly obtained without necessity of the offset canceling circuit.

Operation relating to the timing of switching the output of the voltage follower circuit 72 and the output of the DAC 70 will be described with reference to Fig. 7 in the case where 90% or more of the necessary grayscale voltage is charged in the liquid crystal capacitance 25, and the voltage difference from the necessary voltage is set within the voltage range of

1/2 LSB (least significant bit).

Fig. 7 is an enlarged diagram of the wave form of the voltage applied to a liquid crystal shown in Fig. 3 between the reference voltages V3 and V4.

5 In order to obtain desired display of the liquid crystal, it is assumed, for example, that a voltage VA is necessary as the voltage applied to a liquid crystal. In the embodiment, it is necessary to obtain such a voltage as the voltage applied to a liquid crystal that falls in the range of the voltage VLSB
10 corresponding to 1/2 LSB with respect to the necessary voltage VA (i.e., the range of from voltage VLSB to VA), and is 90% or more of the voltage VA. Fig. 7 shows an example satisfying the voltage in VAD corresponding to 90% of the necessary voltage VA, where the voltage VLSB within the range of the voltage
15 (LSB)/2 with respect to the voltage VA is charged within the first period t1, and it is charged to the voltage VA within the second period t2.

According the configuration, the necessary liquid crystal display is ensured, and the shortage in voltage is
20 compensated by the output of DAC 70 to obtain a highly accurate output voltage within the select period t.

With respect to the switching timing of switching the output of the voltage follower 72 and the output of the voltage output source 70, it is considered that the point, at which the
25 grayscale voltage is ensured to a certain extent, is set as the switching timing.

Second Embodiment

Fig. 8 shows a modified example of the voltage supplying device having the constitution shown in Fig. 5.

As shown in Fig. 8, the voltage supplying device has such a constitution that a first control signal generation circuit 74 for controlling a first switching element Q1 and a second control signal generation circuit 75 for controlling a second switching element Q2, and the first switching element Q1 and the second switching element Q2 are independently controlled.

Fig. 9 shows the wave form of the embodiment shown in Fig. 8.

In Fig. 9, the first switching element Q1 is turned on by a control signal CNT1 output from a data driver IC 30 in synchronized with the latch pulses LP, and the second switching element Q2 is turned off by a control signal CNT2. At this time, the control signal CNT2 is controlled in such a manner that periods θ are present where both the first switching element Q1 and the second switching element Q2 are off.

The output of the voltage follower 72 is switched to the output of the DAC 70 by the control signals CNT1 and CNT2, so as to exhibit the wave form of the voltage applied to a liquid crystal shown by output VY2.

According to the constitution shown in Fig. 8, the first switching element Q1 and the second switching element Q2 are prevented from turning on at the same time. Furthermore, according to the constitution, such a phenomenon can be prevented from occurring that the output of the voltage follower

circuit 72 is returned to the non-inverse input terminal 201 of the voltage follower circuit 72 through the second switching element Q2 to cause oscillation.

5 Third Embodiment

In the circuit shown in Fig. 10, a third switching element Q3 is provided between the power source terminals of the voltage follower circuit 72, in addition to the circuit shown in Fig. 5. The third switching element Q3 is controlled by the control signal CNT1 in synchronized with the first switching element Q1. The operation of the DAC 70 and the voltage follower circuit 72 is the same as the circuit shown in Fig. 5.

When the output of the voltage follower circuit 72 is switched to the output of the DAC 70, the first switching element Q1 is turned off to cut off the output of the voltage follower circuit 72. The third switching element Q3 is then turned off in synchronized with the timing of turning the first switching element Q1 off, so as to cut off the power source supply to the voltage follower circuit 72.

According to the configuration, the power source supply is cut off in the period where the output of the voltage follower circuit 72 is not utilized, whereby the electric power consumption can be reduced.

25 Fourth Embodiment

Examples of the constitution of the voltage follower circuit 72 include the circuit shown in Fig. 12. The circuit

shown in Fig. 12 indicates a circuit of a voltage follower circuit 72 conducting class AB operational amplification, which is mainly composed of a differential amplifier 91, an output amplifier 92 and an input section 93. The circuit of Fig. 12 is constituted by N type MOS transistors QN1 to QN31 and P type MOS transistors QP1 to QP31. The voltage supplied from the DAC 70 is input as an input voltage VIN of the input section 93. Amplification in the final stage is conducted in the output amplifier 92 to supply an output voltage VOUT to the load capacitance.

The input and output characteristics of the output voltage VOUT with respect to the input voltage VIN of the voltage follower circuit 72 is shown in Fig. 11.

In the figure, VDD denotes the power source potential of the voltage follower circuit 72, and VEE denotes the ground potential.

In Fig. 11, linear input and output characteristics cannot be obtained within the range of the input voltage VIN of from 0 to VTHN due to the operation of the N type MOS transistor QN31 having the threshold voltage VTHN in the output amplifier 92 in Fig. 12, but saturated output characteristics appears. Similarly, linear input and output characteristics cannot be obtained within the range of the input voltage VIN of from (VDD + VTHP) to VDD due to the operation of the P type MOS transistor QP31 having the threshold voltage VTHP (negative voltage) in the output amplifier, but saturated output voltage appears.

In Fig. 12, when the input voltage V_{IN} varies from 0 V to the threshold voltage V_{THN} , the potential of a node 212 as a drain of the P type MOS transistor QP21 connected to a gate of the N type MOS transistor QN31 in the output amplifier 92 becomes lower than the potential of a node 213 as a source. As a result, the N type MOS transistor QN31 functions to turn off in the region lower than the threshold voltage V_{THN} , and the electric current cannot flow. Therefore, the output voltage V_{OUT} is saturated.

When the input voltage V_{IN} varies from $(V_{DD} + V_{THP})$ to the power source potential V_{DD} , the potential of a node 210 as a drain of the N type MOS transistor QN1 connected to a gate of the P type MOS transistor QP31 in the output amplifier 92 becomes higher than the potential of a node 211 as a source. As a result, the P type MOS transistor QP31 functions to turn off in the region higher than the threshold voltage $(V_{DD} + V_{THP})$, and the electric current cannot flow. Therefore, the output voltage V_{OUT} is saturated.

A circuit improved in the input and output characteristics in that the output voltage is saturated due to the threshold voltages V_{THN} and V_{THP} is shown Fig. 13.

The threshold voltages V_{THN} and V_{THP} varies under the influence of a constant current circuit inside the voltage follower circuit 72, in addition to the threshold voltages inherent in the MOS transistor elements. Because a constant electric current flows by N type MOS transistors QN11 and QN12 and P type MOS transistors QP11 and QP12, the voltage

corresponding to the offset is superposed. Therefore, in the embodiment, such threshold voltages V_{THN} and V_{THP} are assumed that consider the voltage corresponding to the offset.

In the circuit shown in Fig. 13, a comparator 76 is added to compare the input voltage at the node 203 and the output voltage at node 204 of the voltage follower circuit 72. Based on the compared result of the comparator 76, a control signal is supplied to the gates of the first switching element Q1 and the second switching element Q2 through the first control signal generation circuit 74.

The comparator 76 compares as to whether the output voltage V_{OUT} at the node 204 falls within the input voltage range $(V_{IN} \pm \Delta V)$ (ΔV : arbitrarily set value of error) at the node 203. The control signal is generated through the first control signal generation circuit 74. According to the operation, the first switching element Q1 is turned off, and the second switching element Q2 is turned on, whereby the output of the DAC 70 becomes the output voltage V_{OUT} . There are cases where the output voltage V_{OUT} is overshoot or undershoot with respect to the input voltage V_{IN} to exceed or underrun the allowable range of the set value of error $\pm \Delta V$. In these cases, the allowable range considering the same $(V_{IN} \pm \Delta V)$ is set, or in alternative, the gain of the output voltage V_{OUT} is set at a large value, and the number of occurrence where the output voltage V_{OUT} crosses a constant voltage is counted, whereby the timing of generating the control signal can be set.

As a modified example of the embodiment, the method of

detection shown in Fig. 14 can be considered.

The voltage supplying device shown in Fig. 14 is constituted by a first comparator 77, a second comparator 78 and an OR circuit 79 contained therein. The input voltage VIN of the voltage follower circuit 72 is compared between the voltage at the node 203 and the reference voltages set in the first comparator 77 and the second comparator 78 to provide a comparison signal, which is then supplied to the OR circuit 79. The OR circuit 79 supplies the control signal to the first switching element Q1 and the second switching element Q2 through the first control signal generation circuit 74 when at least one of the first comparator 77 and the second comparator 78 receives a high level signal.

For example, as the reference voltage of the first comparator 77, an interface point is set where the input voltage VIN at the node 203 becomes the threshold voltage ($V_{DD} + V_{THP}$) in the input and output characteristics of the voltage follower circuit 72 shown in Fig. 11. When a voltage higher than the threshold voltage ($V_{DD} + V_{THP}$) is input, a high level signal is output from the first comparator 77 and supplied to the OR circuit 79. A low level signal is output from the second comparator 78 and supplied to the OR circuit 79. A high level signal is thus output from the OR circuit 79 to generate the control signal through the first control signal generation circuit 74. The first switching element Q1 is turned off, and the second switching element Q2 is turned on, whereby the output of the DAC 70 becomes the output voltage VOUT. Similarly, as

the reference voltage of the second comparator 78, an interface point is set where the input voltage VIN at the node 203 becomes the threshold voltage VTHN in the input and output characteristics of the voltage follower circuit 72 shown in Fig.

11. When a voltage lower than the threshold voltage VTHN is input, a high level signal is output from the second comparator 78, and a low level signal is output from the first comparator 77. A high level signal is output from the OR circuit 79 to generate the control signal through the first control signal generation circuit 74. The first switching element Q1 is turned off, and the second switching element Q2 is turned on, whereby the output of the DAC 70 becomes the output voltage VOUT.

According to the operation, when the output of the comparator 76 is varied in the range of the input voltage of from 0 to VTHN or from (VDD + VTHP) to VDD to cut off the output of the voltage follower circuit 72 at that timing, so as to switch to the output of the DAC 70, the linear output characteristics 223 can be ensured instead of the output characteristics 221 where the output voltage is saturated, or the linear output characteristics 227 can be ensured instead of the output characteristics 225.

In the case where the voltage supplying device 58 is used in a TFT liquid crystal device using the DAC method, an output voltage with high accuracy can be obtained without an offset canceling circuit. Furthermore, an output voltage with high accuracy can be obtained in the range of the input voltage from 0 V to the power source voltage VDD, and thus a voltage of a

wider range can be utilized.

Fifth Embodiment

Fig. 15 shows a circuit containing a third switching
5 element for turning the power source voltage of the voltage
follower circuit 72 on and off, in addition to a voltage
supplying device having the constitution shown in Fig. 13.

As shown in Fig. 15, the power source of the voltage
10 follower circuit 72 itself can be turned off during the period
where the output of the DAC 70 is supplied as the output voltage,
whereby the electric power consumption can be reduced.

The invention can be applied to various kinds of
electronic instrument, such as a portable phone, a game machine,
an electronic organizer, a personal computer, a word processor,
15 a television set and a vehicle navigation system.

Sixth Embodiment

Fig. 16 shows a voltage supplying device according to a
sixth embodiment. Also in Fig. 16, there is provided the
20 voltage follower circuit (a second impedance conversion
circuit) 72 for performing impedance conversion on voltage
selected in a DAC 70 and outputting the converted voltage. The
DAC 70 may include, for example, sixty-four analogue switches
71. One of the analogue switches 71 is turned on based on
25 grayscale data (digital data). The first and the second
switching elements Q1 and Q2 are connected to the voltage
follower circuit 72, and they are turned on or off at timing

described in the above-described embodiments.

In Fig. 16, there is provided a reference voltage generating circuit 300 for generating sixty-four reference voltages V0 to V63 to be supplied to the DAC 70. The reference voltage generating circuit 300 includes a ladder resistor circuit to which at least sixty-five resistors are connected in series. The reference voltage generating circuit 300 outputs sixty-four voltages which have been divided in the ladder resistor circuit as sixty-four gamma-corrected reference voltages. For example, five reference voltages V2, V8, V47, V55 and V61 may be supplied to the reference voltage generating circuit 300 from the reference voltage supplying circuit 310.

Sixty-four voltage follower circuits (first impedance conversion circuits) 320 are provided between the reference voltage generating circuit 300 and the DAC 70. The sixty-four voltage follower circuits 320 perform impedance conversion on sixty-four reference voltages V0 to V63 from the reference voltage generating circuit 300 and supply them to the DAC 70. Each of the voltage follower circuits 320 includes third and fourth switching elements Q3 and Q4 like the voltage follower circuit 72 at the output side of the DAC 70. In other words, the third switching element Q3 blocks the output of the voltage follower circuit 320 while the fourth switching element Q4 forms a bypass route 322 and shorts an input/output line of the voltage follower circuit 320.

In order to generate multiple output voltages V_{OUT} , the

reference voltage generating circuit 300 and the reference voltage supplying circuit 310 are shared, and the DAC 70 and the voltage follower circuits 72 are prepared as many as the output voltages V_{OUT} require.

5 Here, also in the voltage supplying device shown in Fig. 16, the first switching element Q1 is turned on and the second switching element Q2 is turned off so that voltage is output from the voltage follower circuit 72 in the first period t1 as shown in Fig. 6B. For example, if one analogue switch 71 is
10 turned on in the DAC 70 and the voltage V31 is selected, the voltage follower circuit 72 performs impedance conversion on the voltage V31 and outputs the converted voltage (see Fig, 17).

In the first period t1, as shown in Fig. 17, the third switching elements Q3 are turn on and fourth switching elements
15 Q4 are turned off, which are connected to sixty-four voltage follower circuits 320. Thus, the reference voltages V0 to V63 from the reference voltage generating circuit 300 undergo impedance conversion in the voltage follower circuits 320 and are supplied to the DAC 70.

20 The reason why the voltage follower circuit 320 is provided is as follows: First of all, the power consumption is reduced by increasing a total resistant value of the ladder resistor provided in the reference voltage generating circuit 300 so as to reduce current flowing the resister. Assume that
25 300 μ A current flows when the total resistant value of the ladder resistor circuit is 15 k Ω . Then, current is reduced to 250 μ A when the total resistant value is 20 k Ω . As a result, without

the voltage follower circuit 320, the current flowing the DAC 70 is reduced. Since the analogue switch 71 of the DAC 70 has a load capacitance, it is difficult to drive. Accordingly, output current is increased in the voltage follower circuit 320.

5 Next, in a second period t_2 shown in Fig. 6B, the first switching element Q1 is turned off while the second switching element Q2 is turned on. The output of the DAC 70 is directly supplied through the bypass route 205 not passing through the voltage follower circuit 72 (see Fig. 18). As a result, it
10 cancels that output/input offset of the voltage follower circuit 72 affecting the output voltage V_{OUT} .

However, the input/output offset in the voltage follower circuit 320 affects the output voltage V_{OUT} . Thus, in all or parts of the second period t_2 , the third switching element Q3
15 connected to the voltage follower circuit 320 is turned off while the fourth switching element Q4 is turned on so as to form the bypass route 322. Thus, it cancels that the input/output offset of the voltage follower circuit 320 affecting the output voltage V_{OUT} .

20 Here, in an extreme example, the grayscale may be inverted due to the input/output offset in a middle scale area with less grayscale voltage difference. For example, assume that the output voltage V_{OUT} which must be set into the reference voltage V31 is actually set into the voltage V30 or V32 ($V32 < V31 < V30$).
25 According to this embodiment, the voltage V31 can be reset during the second period t_2 . This is because, as shown in Fig. 18, a node B at the output voltage V_{OUT} and a node A at a connecting

point between two resistors R31 and R32 are shorted through the second and the fourth switching elements Q2 and Q4 and the analogue switch 71 of the DAC 70. If the output voltage V_{OUT} is set into the higher voltage V30 or the lower voltage V32 than the actual voltage V31, current flows into the resistor R31 or R32. Then, the output voltage V_{OUT} is returned to the voltage V31.

The voltage at the node A which is the connecting point of the resistors R31 and R32 is always the voltage V31 as far as the upper end of the resistor R31 is the voltage V30 and the lower end of the resistor R32 is the voltage V32. Therefore, the output voltage V_{OUT} connected to the node A between the resistors R31 and R32 is always set into the voltage V31. Even though the total resistance value of the ladder resistor is large, the resistance values of the resistors R31 and R32 are small. Therefore, the output voltage V_{OUT} at the node B is charged or discharged by current flowing the resistor R31 or R32 and then is set into the predetermined voltage V31.

Sixty-four third switching elements Q3 may be turned off and sixty-four fourth switching elements Q4 may be turned on at least during the last part of the second period t_2 . The timing is not limited to the entire period of the second period t_2 .

Further, in the device shown in Fig. 16, there are provided fifth switching elements (equivalent to the switching elements Q3 in Fig. 10) for controlling power supply to the voltage follower circuit 72. Each of the fifth switching

elements may be turned on/off in synchronization with the first switching element Q1. Similarly, there are provided sixth switching elements (not shown) for controlling power supply to sixty-four voltage follower circuits 320. Each of the sixth
5 switching elements can be turned on/off in synchronization with the third switching element Q3 shown in Fig. 16. When the bypass 322 shown in Fig. 16 is formed, the power consumption can be reduced by blocking the power supply to the voltage follower circuit 320. In this point of view, the third switching element
10 Q3 connected to the voltage follower circuit 320 may be turned off and the fourth switching element Q4 may be turned on before the second period t_2 starts. This is for increasing the effect of the low power consumption.

15 Seventh Embodiment

Fig. 19 shows an example of the reference voltage supplying circuit 310 shown in Fig. 16. The reference voltage supplying circuit 310 can supply six reference voltages V2, V8, V16, V47, V55 and V61 from the outside or through resistance
20 division. Thus, the reference voltage supplying circuit 310 includes six input terminals VR0 to VR5 to which external reference voltages are input. Further, the reference voltage supplying circuit 310 has a ladder resistor 312 to which multiple resistors R are connected in series and multiple
25 switches SW which are connected to the multiple resistors R, respectively. If the external reference voltages V2, V8, V16, V47, V55 and V61 are input to the input terminals VR0 to VR5,

all of the switches SW are turned off. Otherwise, one switch SW in each group including four switches is turned on. Thus, six reference voltages V2, V8, V16, V47, V55 and V61 generated through the resistance division are output from the reference voltage supplying circuit 310. The gamma-correction characteristic can be changed by making the six reference voltages V2, V8, V16, V47, V55 and V61 variable.

At the latter part of the reference voltage supplying circuit 310, six voltage follower circuits (first impedance conversion circuits) 330 are provided. Further, one switching element (third switching elements) SW1 is provided between each of the voltage follower circuits 330 and the reference voltage circuit 300. That is, there are six switching elements SW1 in total. Further, there are provided six switching elements (fourth switching elements) for shorting each input/output line of six voltage follower circuits 330.

The reason why six voltage follower circuits 330 are provided are to increase the total resistant value of the ladder resistant circuit 312 so as to reduce the current flowing therein as well as to perform current amplification on six reference voltages V2, V8, V16, V47, V55 and V61 which are generated through resistance division.

Therefore, when the reference voltage generated through the resistance division, rather than external reference voltage, is used, the switching element SW1 is turned off and the switching element SW2 is turned on. Then, the voltage follower circuit 320 is used. Conversely, when the external reference

voltage is input, the current amplification is not always necessary. Thus, the switching element SW1 is turned on and the switching element SW2 is turned off. As a result, the external reference voltage may be supplied through the bypass route 332, not through the voltage follower circuit 330.

Also when the external reference voltage is used, the switching element SW1 is turned off and the switching element SW2 is turned on. Then, the current amplification may be performed in the voltage follower circuit 330. In this case, the bypass route 332 may be formed so as to monitor voltage in the output stage of the voltage follower circuit 330.

The invention can be applied to various kinds of electronic instrument, such as a portable phone, a game machine, an electronic organizer, a personal computer, a word processor, a television set and a vehicle navigation system.